

INCREMENTAL REDUNDANCY TRANSMISSION FOR MULTIPLE PARALLEL CHANNELS IN A MIMO COMMUNICATION SYSTEM

[0001] This application claims the benefit of provisional U.S. Application Serial No. 60/501,776, entitled "H-ARQ for MIMO Systems with Successive Interference Cancellation," filed September 9, 2003 and U.S. Application Serial No. 60/531,393, entitled "Incremental Redundancy Transmission for Multiple Parallel Channels in a MIMO Communication System," filed December 19, 2003 assigned to the assignee of the present application, and incorporated herein by reference in its entirety for all purposes.

BACKGROUND

I. Field

[0002] The present invention relates generally to communication, and more specifically to techniques for transmitting data on multiple parallel channels in a multiple-input multiple-output (MIMO) communication system.

II. Background

[0003] A MIMO system employs multiple (N_T) transmit antennas and multiple (N_R) receive antennas for data transmission and is denoted as an (N_T, N_R) system. A MIMO channel formed by the N_T transmit and N_R receive antennas may be decomposed into N_S spatial channels, where $N_S \leq \min \{N_T, N_R\}$, as described below. N_S data streams may be transmitted on the N_S spatial channels. The MIMO system can provide increased transmission capacity if the N_S spatial channels created by the multiple transmit and receive antennas are used for data transmission.

[0004] A major challenge in a MIMO system is selecting suitable rates for data transmission on the MIMO channel based on channel conditions. A "rate" may indicate a particular data rate or information bit rate, a particular coding scheme, a particular modulation scheme, a particular data packet size, and so on. The goal of the rate selection is to maximize the overall throughput on the N_S spatial channels while meeting certain quality objectives, which may be quantified by a target packet error rate (e.g., 1% PER) or some other measures.

[0005] The transmission capacity of each spatial channel is dependent on the signal-to-noise-and-interference ratio (SINR) achieved by that spatial channel. The SINRs for the N_S spatial channels are dependent on the channel conditions and may further be dependent on the manner in which the data streams are recovered at the receiver. In one conventional MIMO system, a transmitter encodes, modulates, and transmits each data stream in accordance with a rate selected based on a model of a static MIMO channel. Good performance can be achieved if the model is accurate and if the MIMO channel is relatively static (i.e., does not change much over time). In another conventional MIMO system, a receiver estimates the MIMO channel, selects a suitable rate for each spatial channel based on the channel estimates, and sends N_S selected rates for the N_S spatial channels to the transmitter. The transmitter then processes N_S data streams in accordance with the selected rates and transmits these streams on the N_S spatial channels. The performance of this system is dependent on the nature of the MIMO channel and the accuracy of the channel estimates.

[0006] For both conventional MIMO systems described above, the transmitter processes and transmits each data packet for each spatial channel at the rate selected for that spatial channel. The receiver decodes each data packet received on each spatial channel and determines whether the packet is decoded correctly or in error. The receiver may send back an acknowledgment (ACK) if the packet is decoded correctly or a negative acknowledgment (NAK) if the packet is decoded in error. The transmitter may retransmit each data packet decoded in error by the receiver, in its entirety, upon receiving a NAK for the packet.

[0007] The performance of both MIMO systems described above is highly dependent on the accuracy of the rate selection. If the selected rates for the spatial channels are too conservative (e.g., because the actual SINRs are much better than the SINR estimates), then excessive system resources are expended to transmit data packets and channel capacity is underutilized. Conversely, if the selected rates for the spatial channels are too aggressive, then the data packets may be decoded in error by the receiver and system resources may be expended to retransmit these packets. Rate selection for a MIMO system is challenging because of (1) greater complexity in the channel estimation for a MIMO channel, (2) the time-varying and independent nature of the spatial channels, and (3) interaction among the multiple data streams transmitted on the spatial channels.

[0008] There is therefore a need in the art for techniques to efficiently transmit data on multiple spatial channels in a MIMO system and which do not require accurate rate selection in order to achieve good performance.

SUMMARY

[0009] Techniques for performing incremental redundancy (IR) transmission on multiple (N_D) parallel channels in a MIMO system are provided herein. These parallel channels may be formed (1) by the multiple spatial channels in the MIMO system, (2) in a manner such that they achieve similar SINRs, or (3) in some other manners. Initially, a receiver or a transmitter in the MIMO system estimates the SINRs for the N_D parallel channels and selects N_D rates for these parallel channels. The SINRs may be dependent on various factors such as the transmission scheme used by the transmitter, the processing performed by the receiver, and so on. The transmitter is provided with the selected rates if the receiver performs the rate selection.

[0010] The transmitter processes (e.g., encodes, partitions, interleaves, and modulates) each data packet for each parallel channel based on the rate selected for that channel and obtains multiple (N_B) data symbol blocks for the packet. The first data symbol block typically contains sufficient information to allow the receiver to recover the data packet under favorable channel conditions. Each of the remaining data symbol blocks contains additional redundancy to allow the receiver to recover the data packet under less favorable channel conditions. For each data packet, the transmitter transmits one data symbol block at a time until all blocks for the packet are transmitted. The transmitter terminates the transmission of a data packet early if the packet is recovered (i.e., decoded successfully) by the receiver with fewer than all data symbol blocks.

[0011] The receiver performs detection on N_R sequences of received symbols and obtains a detected symbol block for each data symbol block transmitted by the transmitter. The subsequent processing is dependent on whether the parallel channels are independent or inter-dependent.

[0012] The N_D parallel channels are independent if data transmission on each parallel channel is independent of data transmission on other parallel channels. In this case, for each data packet on each parallel channel, the receiver processes (e.g., demodulates, deinterleaves, re-assembles, and decodes) all detected symbol blocks obtained for the data packet and provides a decoded packet. The receiver may send

back an ACK if the decoded packet is good and a NAK if the decoded packet is in error. The receiver terminates the processing for each data packet that is recovered or if all data symbol blocks have been received for the packet.

[0013] The N_D parallel channels are inter-dependent if data transmission on each parallel channel is dependent on data transmission on other parallel channels. This is the case if the receiver uses a “successive interference cancellation” (SIC) processing technique to obtain the detected symbol blocks. With SIC, whenever a data packet is recovered on a parallel channel, the interference this packet causes to not yet recovered data packets on other parallel channels is estimated and canceled prior to performing the detection to obtain the detected symbol blocks for these other data packets. The SINRs for later recovered data packets are thus higher, and higher rates may be selected for these packets. The data packets are then recovered by the receiver in a particular order, determined based on their selected rates, so that the SINRs needed to recover these data packets can be attained.

[0014] For an “ordered” SIC transmission scheme, if a data packet on a given parallel channel x is recovered earlier than expected, then one of several options are available. First, the transmitter can transmit nothing on parallel channel x and use more or all transmit power for the data packets not yet recovered. Second, the transmitter can transmit a new “short” data packet on parallel channel x . The short packet is expected to be recovered at or before the next data packet to be recovered. Third, the transmitter can transmit a new “long” data packet on parallel channel x . The long packet is expected to be recovered after the next data packet to be recovered. One of these options may be selected based on a metric that compares throughputs with and without packet transmission on parallel channel x after the early termination.

[0015] For a “cycled” SIC transmission scheme, whenever a data packet is recovered for a parallel channel, the transmitter transmits a new data packet on this parallel channel, and the receiver cycles to the next parallel channel and attempts to recover a data packet on this next parallel channel.

[0016] The SIC and other transmission schemes are described below. Various aspects and embodiments of the invention are also described in further detail below.

BRIEF DESCRIPTION OF THE DRAWINGS

[0017] The features and nature of the present invention will become more apparent from the detailed description set forth below when taken in conjunction with the drawings in which like reference characters identify correspondingly throughout and wherein:

- [0018] FIG. 1 shows a block diagram of a transmitter and a receiver in a MIMO system that implements IR transmission for multiple (N_D) parallel channels;
- [0019] FIG. 2 shows a process for performing IR transmissions for parallel channels;
- [0020] FIG. 3 illustrates IR transmission for one data stream on one parallel channel;
- [0021] FIG. 4 shows a transmission scheme for a MIMO-OFDM system;
- [0022] FIG. 5 illustrates IR transmission for N_D independent parallel channels;
- [0023] FIGS. 6A through 6C illustrate the ordered SIC transmission scheme with three different options for early termination of a data packet on one parallel channel;
- [0024] FIG. 7 shows plots of PER for Packet 1b and Packet 2a versus number of transmission cycles for Packet 2a;
- [0025] FIG. 8 shows a state diagram for the ordered SIC transmission scheme;
- [0026] FIGS. 9A and 9B illustrate the cycled SIC transmission scheme;
- [0027] FIG. 10 shows a transmit (TX) data processor at the transmitter;
- [0028] FIG. 11 illustrates the processing of one data packet by the transmitter;
- [0029] FIG. 12 shows a TX spatial processor and a transmitter unit at the transmitter;
- [0030] FIG. 13 shows one embodiment of the receiver;
- [0031] FIG. 14 shows a receive (RX) data processor at the receiver in FIG. 13; and
- [0032] FIG. 15 shows a receiver that implements the SIC technique.

DETAILED DESCRIPTION

[0033] The word “exemplary” is used herein to mean “serving as an example, instance, or illustration.” Any embodiment or design described herein as “exemplary” is not necessarily to be construed as preferred or advantageous over other embodiments or designs.

[0034] For a MIMO system, N_D data streams may be transmitted simultaneously on N_D parallel channels, one data stream on each parallel channel, where $N_D > 1$. Each parallel channel may correspond to a spatial channel or may be formed in some other

manner, as described below. Each data stream may be processed independently based on a rate selected for that data stream and transmitted on its parallel channel.

[0035] FIG. 1 shows a block diagram of a transmitter 110 and a receiver 150 in a MIMO system 100 that implements IR transmission for multiple data streams on multiple parallel channels. At transmitter 110, a TX data processor 120 receives N_D data streams from a data source 112. TX data processor 120 processes (e.g., formats, encodes, partitions, interleaves, and modulates) each data packet in each data stream in accordance with a rate selected for that data stream and provides N_B data symbol blocks for the packet, where $N_B > 1$ and may be dependent on the selected rate. Each data symbol block can be transmitted in one time slot (or simply, “slot”), which is a predetermined time period for MIMO system 100. The selected rate for each data stream may indicate the data rate, coding scheme or code rate, modulation scheme, packet size, number of data symbol blocks, and so on, which are indicated by the various controls provided by a controller 140. The selected rate for each data stream may be static or continually updated (e.g., based on channel conditions). For IR transmission of a given data stream, the data symbol blocks for each data packet of that data stream are transmitted one block at a time until the packet is recovered by receiver 150 or all blocks have been transmitted.

[0036] A TX spatial processor 130 receives N_D data symbol streams from TX data processor 120. Each data symbol stream includes a set of data symbol blocks for each data packet in the corresponding data stream. TX spatial processor 130 performs processing (e.g., demultiplexing, spatial processing, and so on) to transmit the N_D data symbol streams from N_T transmit antennas. Various transmission schemes may be implemented, as described below. Depending on the transmission scheme selected for use, up to N_D data symbol blocks for up to N_D data streams are transmitted simultaneously on up to N_D parallel channels in any given slot. TX spatial processor 130 also multiplexes in pilot symbols, which are used for channel estimation by receiver 150, and provides N_T transmit symbol streams to a transmitter unit (TMTR) 132.

[0037] Transmitter unit 132 receives and conditions (e.g., converts to analog, frequency upconverts, filters, and amplifies) the N_T transmit symbol streams to obtain N_T modulated signals. Each modulated signal is then transmitted from a respective transmit antenna (not shown in FIG. 1) and via the MIMO channel to receiver 150. The MIMO channel distorts the N_T transmitted signals with a MIMO channel response and

further degrades the transmitted signals with additive white Gaussian noise and possibly interference from other transmitters.

[0038] At receiver 150, the N_T transmitted signals are received by each of N_R receive antennas (not shown in FIG. 1), and the N_R received signals from the N_R receive antennas are provided to a receiver unit (RCVR) 154. Receiver unit 154 conditions, digitizes, and pre-processes each receive signal to obtain a received symbol stream. Receiver unit 154 provides N_R received symbol streams (for data) to an RX spatial processor 160 and received pilot symbols (for pilot) to a channel estimator 172. RX spatial processor 160 processes (e.g., detects, multiplexes, demultiplexes, and so on) the N_R received symbol streams to obtain N_D detected symbol streams, which are estimates of the N_D data symbol streams sent by transmitter 110.

[0039] An RX data processor 170 receives and processes the N_D detected symbol streams to obtain N_D decoded data streams, which are estimates of the N_D data streams sent by transmitter 110. For each data packet of each data stream, RX data processor 170 processes (e.g., demodulates, deinterleaves, re-assembles, and decodes) all data symbol blocks received for that data packet in accordance with the selected rate and provides a decoded packet, which is an estimate of the data packet. RX data processor 170 also provides the status of each decoded packet, which indicates whether the packet is decoded correctly or in error.

[0040] Channel estimator 172 processes the received pilot symbols and/or received data symbols to obtain channel estimates (e.g., channel gain estimates and SINR estimates) for the N_D parallel channels. A rate selector 174 receives the channel estimates and selects a rate for each of the N_D parallel channels. A controller 180 receives the N_D selected rates from rate selector 174 and the packet status from RX data processor 170 and assembles feedback information for transmitter 110. The feedback information may include the N_D selected rates, ACKs and NAKs for the decoded packets, and so on. The feedback information is processed by a TX data/spatial processor 190, further conditioned by a transmitter unit 192, and transmitted via a feedback channel to transmitter 110.

[0041] At transmitter 110, the signal(s) transmitted by receiver 150 are received and conditioned by a receiver unit 146 and further processed by an RX spatial/data processor 148 to obtain the feedback information sent by receiver 150. Controller 140 receives the feedback information, uses the ACKs/NAKs to control the IR transmission

of current data packets being sent on the N_D parallel channels, and uses the N_D selected rates to process new data packets to be sent on the N_D parallel channels.

[0042] Controllers 140 and 180 direct the operation at transmitter 110 and receiver 150, respectively. Memory units 142 and 182 provide storage for program codes and data used by controllers 140 and 180, respectively. Memory units 142 and 182 may be internal to controllers 140 and 180, as shown in FIG. 1, or external to these controllers. The processing units shown in FIG. 1 are described in detail below.

[0043] FIG. 2 shows a flow diagram of a process 200 for performing IR transmissions for N_D data streams on N_D parallel channels in the MIMO system. Initially, the receiver estimates the N_D parallel channels based on pilot and/or data symbols received from the transmitter (step 210). The receiver selects a rate for each of the N_D parallel channels based on the channel estimates and sends N_D selected rates to the transmitter (step 212). The transmitter receives N_D selected rates and processes data packets for the N_D data streams in accordance with the N_D selected rates to obtain N_D data symbol streams (step 220). The transmitter may format, encode, partition, interleave, and modulate each data packet of each data stream in accordance with the rate selected for that data stream to obtain N_B data symbol blocks for the data packet. The transmitter then transmits N_D data symbol streams on N_D parallel channels (step 222). For example, the transmitter may transmit one data symbol block at a time for each data packet of each data stream until all data symbol blocks are transmitted or an ACK is received for the data packet. Various transmission schemes may be used for IR transmission of N_D data streams, as described below.

[0044] The receiver receives the N_D data symbol streams from the transmitter via N_R receive antennas and processes N_R received symbol streams to obtain N_D detected symbol streams (step 230). The receiver then processes the N_D detected symbol streams and recovers the data packets transmitted by the transmitter (step 232). For each slot, the receiver may attempt to recover the current data packet being transmitted for each of the N_D data streams. For example, whenever a new detected symbol block is obtained for a data packet, the receiver may demodulate, deinterleave, re-assemble, and decode all detected symbol blocks received for that packet to obtain a decoded packet. The receiver also checks each decoded packet to determine whether the packet is decoded correctly (good) or in error (erased) (also step 232).

[0045] The ACK/NAK feedback may be achieved in various manners. In one embodiment, the receiver sends a NAK for each decoded packet that is erased, and the transmitter uses this feedback to transmit the next data symbol block for the erased packet. In another embodiment, the transmitter sends one data symbol block at a time for each data packet until an ACK is received for the packet from the receiver (the receiver may or may not send back NAKs). In any case, the receiver terminates the processing for each data packet that is recovered or if all data symbol blocks have been received for the packet (step 234).

[0046] FIG. 2 shows a specific embodiment of IR transmission for N_D data streams on N_D parallel channels. IR transmission for multiple parallel channels may also be performed in other manners, and this is within the scope of the invention.

[0047] FIG. 3 illustrates IR transmission for one data stream (denoted as Stream i) on one parallel channel (denoted as Channel i). The receiver estimates Channel i , selects a rate $r_{i,1}$ for Channel i based on the channel estimates, and sends the selected rate to the transmitter in slot 0. The transmitter receives the selected rate, processes a data packet (Packet 1) for Stream i in accordance with the selected rate, and transmits the first data symbol block (Block 1) for Packet 1 in slot 1. The receiver receives and processes Block 1, determines that Packet 1 is decoded in error, and sends back a NAK in slot 2. The transmitter receives the NAK and transmits the second data symbol block (Block 2) for Packet 1 in slot 3. The receiver receives Block 2, processes Blocks 1 and 2, determines that Packet 1 is still decoded in error, and sends back a NAK in slot 4. The block transmission and NAK response may repeat any number of times. In the example shown in FIG. 3, the transmitter receives a NAK for data symbol block $N_x - 1$ and transmits data symbol block N_x (Block N_x) for Packet 1 in slot m , where N_x is less than or equal to the total number of blocks for Packet 1. The receiver receives Block N_x , processes all N_x data symbol blocks received for Packet 1, determines that the packet is decoded correctly, and sends back an ACK in slot $m + 1$. The receiver also estimates Channel i , selects a rate $r_{i,2}$ for the next data packet for Stream i , and sends the selected rate to the transmitter in slot $m + 1$. The transmitter receives the ACK for Block N_x and terminates the transmission of Packet 1. The transmitter also processes the next data packet (Packet 2) in accordance with the selected rate $r_{i,2}$ and transmits the first data symbol block for Packet 2 in slot $m + 2$. The processing at the transmitter and receiver for Packet 2 continues in the same manner described for Packet 1.

[0048] For the embodiment shown in FIG. 3, there is a delay of one slot for the ACK/NAK response from the receiver for each block transmission. To improve channel utilization, multiple data packets may be transmitted for each data stream in an interlaced manner. For example, one data packet may be transmitted in odd-numbered slots and another data packet may be transmitted in even-numbered slots. More than two data packets may also be interlaced if the ACK/NAK delay is longer than one slot.

[0049] The N_D parallel channels in the MIMO system may be formed in various manners, as described below. Moreover, depending on the processing performed at the receiver, the N_D parallel channels may be independent of one another or inter-dependent. For independent parallel channels, the IR transmission for each data stream may be performed independent of, and without regard to, the IR transmission for the other data streams. For inter-dependent parallel channels, the IR transmission for each data stream is dependent on the IR transmission for the other data streams.

1. IR Transmission for Multiple Independent Parallel Channels

[0050] Various transmission schemes may be used to transmit N_D data streams simultaneously on N_D parallel channels, where $N_D > 1$. Some exemplary transmission schemes are described below. For simplicity, the following description assumes a full rank MIMO channel and $N_D \leq N_S = N_T \leq N_R$.

[0051] In a first transmission scheme, one data stream is transmitted from each of the N_T transmit antennas, without any spatial processing at the transmitter. The model for this transmission scheme may be expressed as:

$$\underline{\mathbf{r}}_{nsp} = \underline{\mathbf{H}}\underline{\mathbf{s}} + \underline{\mathbf{n}} \quad , \quad \text{Eq (1)}$$

where $\underline{\mathbf{s}}$ is an $\{N_T \times 1\}$ data vector with N_T entries for data symbols;

$\underline{\mathbf{r}}_{nsp}$ is an $\{N_R \times 1\}$ receive vector with N_R entries for N_R received symbols obtained via the N_R receive antennas;

$\underline{\mathbf{H}}$ is an $\{N_R \times N_T\}$ channel response matrix for the MIMO channel; and

$\underline{\mathbf{n}}$ is a vector of additive white Gaussian noise (AWGN).

The vector $\underline{\mathbf{s}}$ includes N_T entries for the N_T transmit antennas, with N_D entries being set to N_D data symbols for the N_D data streams and the remaining $N_T - N_D$ entries being

set to zero. The vector \mathbf{n} is assumed to have zero mean and a covariance matrix of $\mathbf{\Lambda}_n = \sigma^2 \mathbf{I}$, where σ^2 is the variance of the noise and \mathbf{I} is the identity matrix with ones along the diagonal and zeros everywhere else.

[0052] Due to scattering in the MIMO channel, the N_D data streams transmitted from the N_T transmit antennas interfere with each other at the receiver. A data stream transmitted from a given transmit antenna may be received by all N_R receive antennas at different amplitudes and phases. The received signal for each receive antenna would then include a component of each of the N_D data streams.

[0053] The receiver may estimate the data vector \mathbf{s} based on various spatial and space-time processing (i.e., “detection”) schemes. For example, the receiver may estimate the data vector \mathbf{s} with a maximal ratio combining (MRC) detector, a minimum mean square error (MMSE) detector, a linear zero-forcing (ZF) detector (which is also referred to as a channel correlation matrix inversion (CCMI) detector), an MMSE linear equalizer, a decision feedback equalizer, or some other detector/equalizer. The spatial processing for some of these detectors is described below.

[0054] The spatial processing for an MRC detector may be expressed as:

$$\hat{\mathbf{s}}_{mrc} = \mathbf{W}_{mrc}^H \mathbf{r}_{nsp} \quad , \quad \text{Eq (2)}$$

where \mathbf{W}_{mrc} is the response of the MRC detector, which is $\mathbf{W}_{mrc} = \mathbf{H}$;

$\hat{\mathbf{s}}_{mrc}$ is an $\{N_T \times 1\}$ vector of N_T detected symbols from the MRC detector; and “ H ” denotes the conjugate transpose.

[0055] The spatial processing for an MMSE detector may be expressed as:

$$\hat{\mathbf{s}}_{mmse} = \mathbf{W}_{mmse}^H \mathbf{r}_{nsp} \quad , \quad \text{Eq (3)}$$

where $\mathbf{W}_{mmse} = (\mathbf{H}\mathbf{H}^H + \sigma^2 \mathbf{I})^{-1} \mathbf{H}$ for the MMSE detector.

[0056] The spatial processing for a zero-forcing detector may be expressed as:

$$\hat{\mathbf{s}}_{zf} = \mathbf{W}_{zf}^H \mathbf{r}_{nsp} \quad , \quad \text{Eq (4)}$$

where $\mathbf{W}_{zf} = \mathbf{H}(\mathbf{H}^H \mathbf{H})^{-1}$ for the zero-forcing detector. For the first transmission scheme, each spatial channel corresponds to a respective transmit antenna.

[0057] In a second transmission scheme, one data stream is transmitted on each “eigenmode” of the MIMO channel. The channel response matrix $\underline{\mathbf{H}}$ may be decomposed using either singular value decomposition or eigenvalue decomposition to obtain N_S eigenmodes of the MIMO channel. The N_S eigenmodes of the MIMO channel are orthogonal to one another, and improved performance may be attained by transmitting multiple data streams via these eigenmodes. The singular value decomposition of the channel response matrix $\underline{\mathbf{H}}$ may be expressed as:

$$\underline{\mathbf{H}} = \underline{\mathbf{U}} \underline{\Sigma} \underline{\mathbf{V}}^H, \quad \text{Eq (5)}$$

where $\underline{\mathbf{U}}$ is an $\{N_R \times N_R\}$ unitary matrix of left eigenvectors of $\underline{\mathbf{H}}$;

$\underline{\Sigma}$ is an $\{N_R \times N_T\}$ diagonal matrix of singular values of $\underline{\mathbf{H}}$; and

$\underline{\mathbf{V}}$ is an $\{N_T \times N_T\}$ unitary matrix of right eigenvectors of $\underline{\mathbf{H}}$.

A unitary matrix is characterized by the property $\underline{\mathbf{M}}^H \underline{\mathbf{M}} = \underline{\mathbf{I}}$. The unitary matrices $\underline{\mathbf{V}}$ and $\underline{\mathbf{U}}$ are used for spatial processing by the transmitter and receiver, respectively, to transmit N_D data streams on the N_S eigenmodes of the MIMO channel.

[0058] The transmitter performs spatial processing with the matrix $\underline{\mathbf{V}}$, as follows:

$$\underline{\mathbf{x}}_{svd} = \underline{\mathbf{V}} \underline{\mathbf{s}}, \quad \text{Eq (6)}$$

where $\underline{\mathbf{x}}_{svd}$ is an $\{N_T \times 1\}$ vector with N_T entries for N_T transmit symbols sent from the N_T transmit antennas. The receive vector is then given as: $\underline{\mathbf{r}}_{svd} = \underline{\mathbf{H}} \underline{\mathbf{V}} \underline{\mathbf{s}} + \underline{\mathbf{n}}$. The receiver performs spatial processing with the matrix $\underline{\mathbf{U}}$, as follows:

$$\underline{\hat{\mathbf{s}}}_{svd} = \underline{\Sigma}^{-1} \underline{\mathbf{U}}^H \underline{\mathbf{r}}_{svd}. \quad \text{Eq (7)}$$

For the second transmission scheme, each spatial channel corresponds to a respective eigenmode. The N_S eigenmodes may be viewed as orthogonal spatial channels obtained through decomposition.

[0059] For the first and second transmission schemes, the N_D data streams may achieve different and possibly widely varying “post-processed” or “post-detection” SINRs, which are the SINRs achieved after linear detection by the receiver (e.g., with

an MMSE, zero-forcing, or MRC detector). Different rates are then needed for the data streams.

[0060] In a third transmission scheme, each of the N_D data streams is transmitted from all N_T transmit symbols such that all data streams experience similar channel conditions and achieve similar post-processed SINRs. The same or similar rates may then be used for the N_D data streams. For this scheme, the transmitter performs matrix multiplication of the data vector \underline{s} with a transmit basis matrix and a diagonal matrix as follows:

$$\underline{x}_{tbn} = \underline{M}\underline{\Lambda}\underline{s} \quad , \quad \text{Eq (8)}$$

where \underline{x}_{tbn} is an $\{N_T \times 1\}$ vector with N_T transmit symbols for the N_T transmit antennas;

\underline{M} is an $\{N_T \times N_T\}$ transmit basis matrix, which is a unitary matrix; and

$\underline{\Lambda}$ is an $\{N_T \times N_T\}$ diagonal matrix.

[0061] The transmit basis matrix \underline{M} allows each data stream to be sent from all N_T transmit antennas and further allows the full power P_{ant} of each transmit antenna to be used for data transmission. The matrix \underline{M} may be defined as $\underline{M} = \frac{1}{\sqrt{N_T}}\underline{E}$, where \underline{E} is

a Walsh-Hadamard matrix. The matrix \underline{M} may also be defined as $\underline{M} = \frac{1}{\sqrt{N_T}}\underline{F}$, where

\underline{F} is a discrete Fourier transform (DFT) matrix with the (m,n) -th entry defined as

$$f_{m,n} = e^{-j2\pi \frac{(m-1)(n-1)}{N_T}} \quad , \quad \text{where } m \text{ is a row index and } n \text{ is a column index for the matrix } \underline{F} \quad ,$$

with $m = 1 \dots N_T$ and $n = 1 \dots N_T$. The diagonal matrix $\underline{\Lambda}$ include N_D non-zero entries along the diagonal and zeros elsewhere. These N_D non-zero entries may be used to allocate different transmit powers to the N_D data streams while conforming to the total transmit power constraint of P_{ant} for each transmit antenna.

[0062] The “effective” channel response observed by the receiver for this transmission scheme is $\underline{H}_{eff} = \underline{H}\underline{M}$. The receiver may estimate the data vector \underline{s} using the MRC, MMSE, zero-forcing, or some other detector/equalizer, where the detector response \underline{W} (which may be \underline{W}_{mrc} , \underline{W}_{mmse} , or \underline{W}_{zf}) is computed with the effective

channel response matrix $\underline{\mathbf{H}}_{eff}$ instead of the channel response matrix $\underline{\mathbf{H}}$. The third transmission scheme is described in detail in commonly assigned U.S. Patent Application Serial No. 10/367,234 entitled "Rate Adaptive Transmission Scheme for MIMO Systems," filed February 14, 2003.

[0063] The third transmission scheme can transmit any number of data streams simultaneously from N_T transmit antennas (i.e., $1 \leq N_D \leq N_S$), allows the N_D parallel channels to achieve similar post-processed SINRs (which can simplify the operation of a SIC receiver), and further allows the same or different transmit powers to be used for the data streams.

[0064] The IR transmission techniques described herein may be implemented in a single-carrier MIMO system that utilizes one carrier for data transmission and a multi-carrier MIMO system that utilizes multiple carriers for data transmission. Multiple carriers may be provided by orthogonal frequency division multiplexing (OFDM), other multi-carrier modulation techniques, or some other constructs. OFDM effectively partitions the overall system bandwidth into multiple (N_F) orthogonal subbands, which are also commonly referred to as tones, bins, or frequency channels. With OFDM, each subband is associated with a respective carrier that may be modulated with data.

[0065] For a MIMO system that implements OFDM (i.e., a MIMO-OFDM system), the N_D data streams may be transmitted on the N_F subbands of the N_T transmit antennas in various manners. For example, each data stream may be transmitted on the N_F subbands of a respective transmit antenna. Alternatively, each data stream may be transmitted on multiple subbands and multiple transmit antennas to achieve frequency and spatial diversity.

[0066] In a fourth transmission scheme, each data stream is transmitted diagonally across the N_F subbands and from all N_T transmit antennas. This scheme provides both frequency and spatial diversity for all N_D data streams transmitted simultaneously and further achieves similar post-processed SINRs for the N_D data streams after linear detection at the receiver.

[0067] **FIG. 4** shows the fourth transmission scheme for a case in which two data streams ($N_D = 2$) are transmitted in an exemplary MIMO-OFDM system with four transmit antennas ($N_T = 4$) and 16 subbands ($N_F = 16$). For the first data stream, the first four data symbols $s_{1,1}$, $s_{1,2}$, $s_{1,3}$ and $s_{1,4}$ are transmitted on subbands 1, 2, 3 and 4,

respectively, of transmit antennas 1, 2, 3 and 4, respectively. The next four data symbols $s_{1,5}$, $s_{1,6}$, $s_{1,7}$ and $s_{1,8}$ wrap around and are transmitted on subbands 5, 6, 7 and 8, respectively, of transmit antennas 1, 2, 3 and 4, respectively. For the second data stream, the first four data symbols $s_{2,1}$, $s_{2,2}$, $s_{2,3}$ and $s_{2,4}$ are transmitted on subbands 1, 2, 3 and 4, respectively, of transmit antennas 3, 4, 1 and 2, respectively. The next four data symbols $s_{2,5}$, $s_{2,6}$, $s_{2,7}$ and $s_{2,8}$ wrap around and are transmitted on subbands 5, 6, 7 and 8, respectively, of transmit antennas 3, 4, 1 and 2, respectively. For the embodiment shown in FIG. 4, not all subbands are used for data transmission and the unused subbands are filled with signal values of zero. The multiplexing/demultiplexing may also be performed in other manners.

[0068] For a MIMO-OFDM system, the spatial processing described above for the transmitter and receiver can be performed for each subband k , for $k = 1 \dots N_F$, based on the channel response matrix $\underline{\mathbf{H}}(k)$ for that subband.

[0069] For a MIMO system that implements orthogonal frequency division multiple access (i.e., a MIMO-OFDMA system), only a subset of the N_F subbands may be available for data transmission to each receiver. The processing described above for the MIMO-OFDM system may also be used for the MIMO-OFDMA system, albeit only on the subbands available for data transmission. For example, the N_D data streams for a given receiver may be transmitted diagonally across the available subbands (instead of all N_F subbands) and from the N_T transmit antennas.

[0070] The N_D parallel channels may be formed in various manners in MIMO and MIMO-OFDM systems. The four transmission schemes described above represent four exemplary methods of forming multiple parallel channels. In general, the parallel channels may be formed using any combination of space, frequency, and time.

[0071] In the following description, a “transmission cycle” (or simply, a “cycle”) is a time period covering the transmission of a data symbol block by the transmitter and the transmission of an NAK/ACK response for that block by the receiver. An “F” denotes decoding failure by the receiver and an “S” denotes decoding success. For simplicity, the interlacing of multiple data packets for each data stream is not shown in the following timing diagrams.

[0072] **FIG. 5** illustrates IR transmission of N_D data streams on N_D independent parallel channels. Because these parallel channels are independent, the receiver can recover each data stream independently and provide an ACK/NAK feedback stream for

that data stream. The transmitter sends a new data symbol block for the current data packet of each data stream in each cycle.

[0073] In the example shown in FIG. 5, for data stream 1 transmitted on parallel channel 1 (Channel 1), the receiver encounters a decoding failure (“F_{1a}”) when attempting to recover data packet 1a (Packet 1a) with just data symbol block 1 in cycle 1, a decoding failure when attempting to recover Packet 1a with data symbol blocks 1 and 2 in cycle 2, a decoding failure when attempting to recover Packet 1a with data symbol blocks 1, 2 and 3 in cycle 3, and a decoding success (“S_{1a}”) when attempting to recover Packet 1a with data symbol blocks 1 through 4 in cycle 4. The transmitter then terminates the transmission of Packet 1a and starts transmitting data symbol blocks for another data packet 1b (Packet 1b). The receiver attempts to recover Packet 1b whenever a new data symbol block is received for that packet, encounters a decoding failure in each of cycles 5 through 8, and is able to correctly decode Packet 1b with data symbol blocks 1 through 5 in cycle 9. The receiver processes each of the other data streams in similar manner, as shown in FIG. 5.

2. IR Transmission for Multiple Interdependent Parallel Channels

[0074] The receiver can process the N_R received symbol streams using the SIC technique to obtain the N_D detected symbol streams. For the SIC technique, which is a non-linear detection scheme, the receiver initially performs detection on the N_R received symbol streams (e.g., using an MRC, MMSE, or zero-forcing detector) and obtains one detected symbol stream. The receiver further processes (e.g., demodulates, deinterleaves, and decodes) this detected symbol stream to obtain a decoded data stream. The receiver then estimates the interference this data stream causes to the other $N_D - 1$ data streams and cancels the estimated interference from the N_R received symbol streams to obtain N_R modified symbol streams. The receiver then repeats the same processing on the N_R modified symbol streams to recover another data stream.

[0075] The receiver thus processes the N_R received symbol streams in N_D successive stages. For each stage, the receiver performs (1) detection on either the N_R received symbol streams or the N_R modified symbol streams from the preceding stage to obtain one detected symbol stream, (2) decodes this detected symbol stream to obtain a corresponding decoded data stream, and (3) estimates and cancels the interference due to this stream to obtain N_R modified symbol streams for the next stage. If the

interference due to each data stream can be accurately estimated and canceled, which requires error-free or low-error recovery of the data stream, then later recovered data streams experience less interference and may be able to achieve higher post-processed SINRs. The SIC technique is described in further detail in commonly assigned U.S. Patent Application Serial No. 09/993,087, entitled "Multiple-Access Multiple-Input Multiple-Output (MIMO) Communication System," filed November 6, 2001.

[0076] For the SIC technique, the post-processed SINR of each data stream is dependent on (1) that stream's SINR with linear detection and without interference cancellation, (2) the particular stage in which the data stream is recovered, and (3) the interference due to later recovered data streams. Thus, even though the N_D data streams may achieve similar post-processed SINRs with linear detection (e.g., using an MMSE, zero-forcing, or MRC detector), these streams will typically achieve different post-processed SINRs with non-linear detection using the SIC technique. In general, the post-processed SINR progressively improves for data streams recovered in later stages because the interference from data streams recovered in prior stages is canceled. This then allows higher rates to be used for later recovered data streams.

[0077] The SIC technique introduces interdependency among the data streams. In particular, the rates for the N_D data streams are selected based on the post-processed SINRs achieved by these data streams, which are in turn dependent on the order in which the data streams are recovered. The post-processed SINR of each data stream assumes that all earlier data streams (i.e., those designated to be recovered prior to that data stream) have been successfully decoded and canceled. The receiver typically needs to recover the N_D data streams in a designated order and normally cannot recover a given data stream until all earlier data streams have been recovered and canceled.

[0078] Various transmission schemes may be used for a MIMO system with a SIC receiver. Several exemplary transmission schemes are described below. For simplicity, the following description assumes two data streams ($N_D = 2$) are transmitted on two parallel channels. However, the concepts described below may be extended to any number of data streams.

A. Ordered SIC Transmission Scheme

[0079] In an ordered SIC transmission scheme, the N_D data streams are recovered in a designated order. For example, the receiver may recover data stream 1 first, then data

stream 2 next, and so on, and data stream N_D last. The designated order may be dependent on the manner in which the data streams are transmitted. For example, the received SINRs for the N_D data streams are likely to be similar for the third and fourth transmission schemes described above. In this case, performance is minimally impacted by the order in which the N_D data streams are recovered, and any order may be selected. The received SINRs for the N_D data streams are likely to be different for the first transmission scheme described above. In this case, better performance may be attained by recovering the data stream with the highest received SINR first, then the data stream with the next highest received SINR, and so on. In any case, for the ordered SIC transmission scheme, the receiver attempts to recover data stream i only after the interference from all earlier data streams 1 to $i - 1$ has been canceled.

[0080] Initially, the post-processed SINRs are estimated for the N_D data streams based on (1) the received SINRs for the data streams, e.g., with equal transmit powers being used for the data streams, and (2) the designated order of recovering the data streams. The post-processed SINR of the data stream recovered in stage ℓ , $\text{SINR}_{pd}(\ell)$, may be expressed as:

$$\text{SINR}_{pd}(\ell) = \frac{1}{\sigma^2 \|\underline{\mathbf{w}}_\ell\|^2}, \quad \text{Eq (9)}$$

where $\underline{\mathbf{w}}_\ell$ is the detector response for the stream recovered in stage ℓ and σ^2 is the variance of the noise at the receiver. The detector response $\underline{\mathbf{w}}_\ell$ is one column of a (e.g., MRC, MMSE, or zero-forcing) detector response $\underline{\mathbf{W}}_\ell$ derived for stage ℓ based on a reduced channel response matrix $\underline{\mathbf{H}}_\ell$ for that stage. The matrix $\underline{\mathbf{H}}_\ell$ is obtained by removing $(\ell - 1)$ columns in the original matrix $\underline{\mathbf{H}}$ corresponding to the data streams already recovered in the $(\ell - 1)$ prior stages. The computation of the post-processed SINR is described in further detail in commonly assigned U.S. Patent Application Serial No. ,entitled “Successive Interference Cancellation Receiver Processing with Selection Diversity,” filed September 23, 2003.

[0081] A rate is selected for each data stream based on its post-processed SINR. The rate selection does not need to be accurate because a data packet can be transmitted with a variable rate with IR transmission. The sizes of the N_D data packets to be transmitted for the N_D data streams are selected, given the selected rates, such that all

data packets are expected to be recovered by the receiver in the same number of cycles (N_{est}), where N_{est} can be determined based on a conservative estimate of the post-processed SINRs. The transmission for each data packet may be terminated early if the packet is recovered prior to cycle N_{est} and may be extended past cycle N_{est} if necessary until the packet is recovered.

[0082] FIGS. 6A through 6C illustrate the ordered SIC transmission scheme with three different transmission options for early termination of a data packet on one data stream. In FIGS. 6A through 6C, two new data packets (Packets 1a and 2a) are transmitted starting in cycle 1 for data streams 1 and 2 on parallel channels 1 and 2 (Channels 1 and 2), respectively. If Packet 1a for data stream 1 is recovered in cycle N_{rec}^1 , which is before cycle N_{est} , then a goal of this transmission scheme is to synchronize both data streams as soon as possible without losing spectral efficiency. Table 1 shows some options available if Packet 1a is recovered before cycle N_{est} .

Table 1

Option	Description
1	Do not transmit anything on Channel 1 and use all transmit power for Packet 2a on Channel 2 after Packet 1a has been recovered, as shown in FIG. 6A. This improves the likelihood of recovering Packet 2a before cycle N_{est} .
2	Transmit a new 'short' data packet on Channel 1, as shown in FIG. 6B. The short packet has a length of N_{short}^1 , where $N_{short}^1 \leq N_{rem}^1$ and $N_{rem}^1 = N_{est} - N_{rec}^1$. The rate for the short packet is selected based on the channel estimates obtained in cycle N_{rec}^1 .
3	Transmit a new 'long' data packet on Channel 1, as shown in FIG. 6C. The long packet has a length of N_{long}^1 , where $N_{long}^1 > N_{rem}^1$. This may delay the recovery of Packet 2a until cycle $N_{rem}^1 + N_{long}^1$, which is the cycle in which the long packet is expected to be recovered.

In Table 1, N_{short}^1 and N_{long}^1 (similar to N_{est}) represent the number of cycles in which the short and long data packets are expected to be recovered, based on a conservative estimate of the post-processed SINRs.

[0083] A metric may be used to select one of the three options shown in Table 1 whenever early termination is encountered. This metric may be defined based on accumulated throughput and defined as follows:

$$R_1(N_{rec}^1, N_{long}^1) > R_2(0, N_{est}) - R_2(0, N_{rec}^1 + N_{long}^1) \quad , \quad \text{Eq (10)}$$

where $R_i(j, n)$ is the accumulated throughput predicted at cycle j for data stream i after n cycles. The left side of the inequality in equation (10) represents the gain in the accumulated throughput ($\Delta R_{1, long}$) for Channel 1 with a new long packet transmitted on Channel 1. The right side of the inequality in equation (10) represents the reduction of the accumulated throughput ($\Delta R_{2, long}$) for Channel 2 because of the new long packet transmission on Channel 1. The term $R_2(0, N_{est})$ denotes the accumulated throughput for Channel 2 if Packet 2a is recovered in cycle N_{est} , as predicted. The term $R_2(0, N_{rec}^1 + N_{long}^1)$ denotes the accumulated throughput for Channel 2 if the transmission for Packet 2a extends to cycle $N_{rec}^1 + N_{long}^1$ because of the long packet transmission on Channel 1. The difference between these two terms represents the reduction in the accumulated throughput for Channel 2. A new long packet may thus be transmitted on Channel 1 if the gain in accumulated throughput for Channel 1 is greater than the reduction in accumulated throughput for Channel 2 (i.e., Option 3 in Table 1 may be selected if equation (10) is true.)

[0084] Equation (10) assumes that N_{est} cycles are needed to recover Packet 2a even if the total transmit power is used for Packet 2a after Packet 1a has been recovered in cycle N_{rec}^1 . This is a pessimistic assumption since the likelihood of recovering Packet 2a before cycle N_{est} improves when higher transmit power is used for Packet 2a after cycle N_{rec}^1 . Equation (10) may be modified as follows:

$$R_1(N_{rec}^1, N_{long}^1) > R_2(0, N_{est}^{power}) - R_2(0, N_{rec}^1 + N_{long}^1) \quad , \quad \text{Eq (11)}$$

where N_{est}^{power} is the number of cycles predicted to be required to recover Packet 2a with all transmit power used for Packet 2a after cycle N_{rec}^1 , where $N_{est}^{power} < N_{est}$.

[0085] FIG. 6A shows IR transmission with null transmission for early termination (Option 1 in Table 1). In FIG. 6A, two new data blocks are transmitted for Packets 1a and 2a on Channels 1 and 2 in each of cycles 1 through N_{rec}^{1a} . For each cycle, the receiver attempts to recover Packet 1a based on all data symbol blocks received for Packet 1a and does not attempt to recover Packet 2a ("X_{2a}"). The receiver encounters

decoding failure (“F_{1a}”) for Packet 1a in each of cycles 1 through $N_{rec}^{1a} - 1$ and decoding success (“S_{1a}”) in cycle N_{rec}^{1a} , which is earlier than cycle N_{est} . The receiver then estimates and cancels the interference due to Packet 1a, attempts to recover Packet 2a, and encounters a decoding failure (“F_{2a}”) for Packet 2a.

[0086] For Option 1, the transmitter uses all transmit power for Packet 2a after Packet 1a has been recovered. For each of cycles $N_{rec}^{1a} + 1$ to N_{rec}^{2a} , the receiver attempts to recover Packet 2a based on all data symbol blocks received for Packet 2a, with the blocks received between cycles 1 through N_{rec}^{1a} having the interference from Packet 1a removed and the blocks received between cycles $N_{rec}^{1a} + 1$ to N_{rec}^{2a} having higher transmit power. The receiver encounters decoding failure (“F_{2a}”) for Packet 2a in each of cycles $N_{rec}^{1a} + 1$ through $N_{rec}^{2a} - 1$ and decoding success (“S_{2a}”) in cycle N_{rec}^{2a} . In this example, Packet 2a is also recovered early, i.e., before cycle N_{est} , because of the higher transmit power used for Packet 2a from cycle $N_{rec}^{1a} + 1$ onward. Two new data packets (Packets 1b and 2b) are then transmitted on Channels 1 and 2 starting in cycle $N_{rec}^{2a} + 1$. The decoding process is repeated on these packets.

[0087] **FIG. 6B** shows IR transmission with short packet transmission for early termination (Option 2 in Table 1). In FIG. 6B, two new data blocks are transmitted for Packets 1a and 2a on Channels 1 and 2 in each of cycles 1 through N_{rec}^{1a} . For each cycle, the receiver attempts to recover Packet 1a and does not attempt to recover Packet 2a. The receiver encounters decoding success (“S_{1a}”) for Packet 1a in cycle N_{rec}^{1a} (which is earlier than cycle N_{est}), estimates and cancels the interference due to Packet 1a, attempts to recover Packet 2a, and encounters a decoding failure (“F_{2a}”) for Packet 2a. A new short Packet 1b with length $N_{short}^{1b} \leq (N_{est} - N_{rec}^{1a})$ is then transmitted on Channel 1 starting in cycle $N_{rec}^{1a} + 1$. For each of cycles $N_{rec}^{1a} + 1$ to $N_{rec}^{1a} + N_{rec}^{1b}$, the receiver attempts to recover Packet 1b based on all data symbol blocks received for Packet 1b and encounters decoding success (“S_{1b}”) in cycle $N_{rec}^{1a} + N_{rec}^{1b}$. In this example, Packet 1b is also recovered before cycle N_{est} . However, no data is transmitted on Channel 1 after cycle $N_{rec}^{1a} + N_{rec}^{1b}$, for example, because the shortest length packet cannot be completely transmitted on Channel 1 prior to cycle N_{est} . The transmitter then uses all transmit power for Packet 2a after Packet 1b has been recovered.

[0088] For each of cycles $N_{rec}^{1a} + N_{rec}^{1b}$ to N_{rec}^{2a} , the receiver attempts to recover Packet 2a based on all data symbol blocks received for Packet 2a, with the blocks received between cycles 1 through N_{rec}^{1a} having the interference from Packet 1a removed, the blocks received between cycles $N_{rec}^{1a} + 1$ to $N_{rec}^{1a} + N_{rec}^{1b}$ having the interference from Packet 1b removed, and the blocks received after cycle $N_{rec}^{1a} + N_{rec}^{1b}$ having higher transmit power. The receiver encounters decoding success (“S_{2a}”) for Packet 2a in cycle N_{rec}^{2a} , which in this example is before cycle N_{est} . Two new data packets are then transmitted on Channels 1 and 2 starting in cycle $N_{rec}^{2a} + 1$.

[0089] FIG. 6C shows IR transmission with long packet transmission for early termination (Option 3 in Table 1). In FIG. 6C, two new data blocks are transmitted for Packets 1a and 2a on Channels 1 and 2 in each of cycles 1 through N_{rec}^{1a} . Upon encountering decoding success (“S_{1a}”) for Packet 1a in cycle N_{rec}^{1a} , a new long Packet 1b with length $N_{long}^{1b} > (N_{est} - N_{rec}^{1a})$ is transmitted on Channel 1 starting in cycle $N_{rec}^{1a} + 1$. For each of cycles $N_{rec}^{1a} + 1$ to $N_{rec}^{1a} + N_{rec}^{1b}$, the receiver attempts to recover Packet 1b based on all data symbol blocks received for Packet 1b and encounters decoding success (“S_{1b}”) in cycle $N_{rec}^{1a} + N_{rec}^{1b}$, which is after cycle N_{est} .

[0090] In cycle N_{rec}^{1a} , the receiver attempts to recover Packet 2a based on all data symbol blocks received for Packet 2a, with the interference from Packet 1a removed, and encounters decoding failure (“F_{2a}”). In cycle $N_{rec}^{1a} + N_{rec}^{1b}$, the receiver attempts to recover Packet 2a based on all data symbol blocks received for Packet 2a, with the blocks received between cycles 1 to N_{rec}^{1a} having the interference from Packet 1a removed and the blocks received between cycles $N_{rec}^{1a} + 1$ to $N_{rec}^{1a} + N_{rec}^{1b}$ having the interference from Packet 1b removed. The receiver encounters decoding success (“S_{2a}”) for Packet 2a in cycle $N_{rec}^{1a} + N_{rec}^{1b}$. Two new data packets are then transmitted on Channels 1 and 2 starting in cycle $N_{rec}^{1a} + N_{rec}^{1b} + 1$.

[0091] The transmission of a new long Packet 1b on Channel 1 may affect the actual rate and the PER achieved for Channel 2. As noted above, N_{est} is the number of cycles predicted for recovering Packet 2a on Channel 2 with the interference from the packet(s) from Channel 1 canceled and for the target PER. If the long Packet 1b on Channel 1 is

recovered in cycle $N_{rec}^{1a} + N_{rec}^{1b}$, which is later than cycle N_{est} , then (1) the rate achieved for Channel 2 decreases from $R_2(0, N_{est})$ to $R_2(0, N_{rec}^{1a} + N_{rec}^{1b})$ and (2) the PER for Packet 2a will be lower than the target PER because more redundancy has been transmitted for Packet 2a. Improved performance may be attained by terminating the transmission for Packet 2a after some predetermined number of cycles (N_{max}^{2a}) and using all transmit power for Packet 1b.

[0092] FIG. 7 shows a plot 710 of the PER for Packet 1b and a plot 712 of the PER for Packet 2a versus number of transmission cycles (N_{trans}^{2a}) for Packet 2a. The target PER is achieved for Packet 2a if it is transmitted for N_{est} cycles (i.e., $N_{trans}^{2a} = N_{est}$), as indicated by point 720. The PER for Packet 2a progressively decreases below the target PER the longer Packet 2a is transmitted past N_{est} cycles, as shown by plot 712. The target PER is achieved for Packet 1b if it is transmitted for N_{long}^{1b} cycles, which occurs at cycle $N_{rec}^{1a} + N_{long}^{1b}$, as indicated by point 722. This assumes that Packet 2a is transmitted during this entire time. The PER for Packet 1b progressively decreases below the target PER the earlier Packet 2a is terminated and all transmit power is used for Packet 1b, as shown by plot 710. The PERs for Packet 1b and 2a cross at cycle N_{sel}^{2a} . If the transmission for Packet 2a is terminated at cycle N_{sel}^{2a} , then the same reliability can be achieved for both Packets 1b and 2a, and the likelihood of recovering Packet 1b before cycle $N_{rec}^{1a} + N_{long}^{1b}$ also improves.

[0093] Alternatively, instead of terminating the transmission of Packet 2a at cycle N_{sel}^{2a} , different transmit powers may be used for Packets 1b and 2a to achieve similar results. For example, N_{long}^{1b} may be selected based on the use of more transmit power for Packet 1b and less transmit power for Packet 2a for the duration of Packet 1b (i.e., from cycles $N_{rec}^{1a} + 1$ to $N_{rec}^{1a} + N_{long}^{1b}$) such that the PERs of Packets 1b and 2a are similar at cycle $N_{rec}^{1a} + N_{long}^{1b}$. As another example, the transmit power for Packet 1b may be progressively increased and the transmit power for Packet 2a may be progressively decreased after cycle N_{est} . Different transmit powers may be used for different data streams using the third or fourth transmission scheme described above.

[0094] Table 2 shows some options available with the transmission of a long Packet 1b that may extend past cycle N_{est} .

Table 2

Option	Description
A	If Packet 1b is recovered before Packet 2a, then any one of the options shown in Table 1 may be selected.
B	Terminate the transmission of Packet 2a after some predetermined number of cycles N_{\max}^{2a} (e.g., $N_{\max}^{2a} = N_{\text{sel}}^{2a}$), wait for Packet 1b to be recovered, then attempt to recover Packet 2a with Packets 1a and 1b canceled.

[0095] FIG. 8 shows an exemplary state diagram 800 that may be maintained by the transmitter and receiver for the ordered SIC transmission scheme. State diagram 800 includes a sync state 810, a new packet transmission state 820, and a null transmission state 830. In sync state 810, two new data packets (Packets 1a and 2a) are transmitted on Channels 1 and 2 starting in the same cycle. These two packets are expected to be recovered in N_{est} cycles if the rate selection is reasonably accurate.

[0096] The state diagram transitions from sync state 810 to new packet transmission state 820 if Packet 1a on Channel 1 is recovered earlier than N_{est} cycles and a new short or long data packet (Packet 1b) is transmitted on Channel 1. In state 820, the receiver attempts to recover Packet 1b on Channel 1 and does not attempt to recover Packet 2a on Channel 2 until Packet 1b is recovered and the interference from Packet 1b is canceled. The state diagram remains in state 820 if Packet 1b is not recovered or if Packet 1b is recovered and a new data packet (Packet 1c) is transmitted on Channel 1. The state diagram transitions from state 820 back to state 810 if the packets on both Channels 1 and 2 are recovered.

[0097] The state diagram transitions from sync state 810 to null transmission state 830 if Packet 1a on Channel 1 is recovered earlier than N_{est} cycles and nothing is transmitted on Channel 1. The state diagram also transitions from state 820 to state 830 if the current packet on Channel 1 is recovered and nothing is transmitted on Channel 1. In state 830, the receiver attempts to recover Packet 2a on Channel 2 with the interference from all packets recovered on Channel 1 canceled. The state diagram remains in state 830 if Packet 2a on Channel 2 is not recovered and transitions back to state 810 if Packet 2a is recovered.

[0098] The ordered SIC transmission scheme can provide good performance if the rate selection is reasonably accurate, so that the recovery of a later data stream is not excessively delayed.

B. Cycled SIC Transmission Scheme

[0099] In a cycled SIC transmission scheme, the N_D data streams are recovered by cycling through the data streams so that the data stream most likely to be decoded correctly is recovered first. Initially, N_D rates are selected for the N_D data streams, and N_D data packets are transmitted on the N_D parallel channels. The rate selection may be crude, and the packet sizes may be selected such that all data packets are expected to be recovered in N_{est} cycles. Whenever a data packet is recovered for a data stream, a new packet is transmitted for that data stream and the receiver attempts to decode a data packet for the next data stream, as described below.

[00100] FIG. 9A shows IR transmission with the cycled SIC transmission scheme. In FIG. 9A, two new data blocks are transmitted starting in cycle 1 for Packets 1a and 2a on Channels 1 and 2. Packet 1a is designated to be recovered first and is processed based on a lower rate due to the interference from Packet 2a. Packet 2a is designated to be recovered later and is processed based on a higher rate achievable with the interference from Packet 1a canceled. Packets 1a and 2a have lengths of N_{est} (i.e., are expected to be recovered in N_{est} cycles). For each cycle, the receiver attempts to recover Packet 1a based on all data symbol blocks received for this packet and does not attempt to recover Packet 2a ("X_{2a}"). The receiver encounters decoding failure ("F_{1a}") for Packet 1a in each of cycles 1 through $N_{rec}^{1a} - 1$ and decoding success ("S_{1a}") in cycle N_{rec}^{1a} . A new Packet 1b is then transmitted on Channel 1 starting in cycle $N_{rec}^{1a} + 1$. Packet 1b has a length of N_{est} and is processed based on a higher rate, which is estimated in cycle N_{rec}^{1a} and under the assumption that the interference from Channel 2 will be canceled.

[00101] In cycle N_{rec}^{1a} , the receiver estimates and cancels the interference due to Packet 1a, attempts to recover Packet 2a, and encounters a decoding failure ("F_{2a}") for Packet 2a. For each of cycles $N_{rec}^{1a} + 1$ to N_{rec}^{2a} , the receiver attempts to recover Packet 2a based on all data symbol blocks received for this packet, with the blocks received in cycles 1 through N_{rec}^{1a} having the interference from Packet 1a removed and the blocks received in cycles $N_{rec}^{1a} + 1$ through N_{rec}^{2a} having the interference from Packet 1b. The receiver encounters decoding failure ("F_{2a}") for Packet 2a in each of cycles $N_{rec}^{1a} + 1$ through $N_{rec}^{2a} - 1$ and decoding success ("S_{2a}") in cycle N_{rec}^{2a} . A new Packet 2b is then

transmitted on Channel 2 starting in cycle $N_{rec}^{2a} + 1$. Packet 2b has a length of N_{est} and is processed based on a higher rate, which is estimated in cycle N_{rec}^{2a} and under the assumption that the interference from Channel 1 will be canceled.

[00102] In cycle N_{rec}^{2a} , the receiver estimates and cancels the interference due to Packet 2a, attempts to recover Packet 1b, and encounters a decoding failure (“F_{1b}”) for Packet 1b. For each of cycles $N_{rec}^{2a} + 1$ to $N_{rec}^{1a} + N_{rec}^{1b}$, the receiver attempts to recover Packet 1b based on all data symbol blocks received for this packet, with the blocks received in cycles $N_{rec}^{1a} + 1$ through N_{rec}^{2a} having the interference from Packet 2a removed and the blocks received in cycles $N_{rec}^{2a} + 1$ through $N_{rec}^{1a} + N_{rec}^{1b}$ having the interference from Packet 2b. The receiver encounters decoding success (“S_{1b}”) for Packet 1b in cycle $N_{rec}^{1a} + N_{rec}^{1b}$. The receiver attempts to recover subsequent packets on Channels 1 and 2 in similar manner.

[00103] FIG. 9B shows the order of recovering the data streams for the cycled SIC transmission scheme. The receiver attempts to recover Packet 1a on Channel 1 in cycles 1 through N_{rec}^{1a} . Upon recovering Packet 1a in cycle N_{rec}^{1a} , the receiver attempts to recover Packet 2a on Channel 2 in cycles $N_{rec}^{1a} + 1$ to N_{rec}^{2a} . Upon recovering Packet 2a in cycle N_{rec}^{2a} , the receiver attempts to recover Packet 1b on Channel 1 in cycles $N_{rec}^{2a} + 1$ to $N_{rec}^{1a} + N_{rec}^{1b}$. The receiver attempts to recover subsequent packets on Channels 1 and 2 in similar manner.

[00104] In general, the receiver can attempt to recover the packets sent on the N_D parallel channels based on the likelihood of recovering these packets. The likelihood of recovering the packet sent on each parallel channel is dependent on various factors such as (1) the post-processed SINR achieved for the parallel channel with linear detection and (2) the number of data symbol blocks already received for the parallel channel. In each cycle, the receiver can attempt to recover only the packet sent on the parallel channel most likely to be recovered in that cycle. Alternatively, the receiver can attempt to recover the packets on all N_D parallel channels, one packet at a time, starting with the parallel channel most likely to be recovered and concluding with the parallel channel least likely to be recovered. If multiple parallel channels have the same

likelihood of being recovered, then the receiver can select one parallel channel (e.g., at a time, in a random manner) for recovery.

[00105] The receiver can cycle through the N_D parallel channels if (1) these channels achieve similar post-processed SINRs with linear detection and (2) the packets for these channels have the same length. As an example, consider a case in which $N_D = 4$ and four new packets are transmitted on four parallel channels starting in cycle 1. In each cycle, the receiver may attempt to recover the packet sent on each parallel channel based on all data symbol blocks received for that packet. The receiver may be able to recover the packet transmitted on, e.g., Channel 2 first, and would then estimate and cancel the interference due to this packet. In each cycle thereafter, the receiver may attempt to recover the packet sent on each of Channels 1, 3, and 4 based on all data symbol blocks received for that packet. The receiver may be able to recover the packet transmitted on, e.g., Channel 3 next, and would then estimate and cancel the interference due to this packet. In each cycle thereafter, the receiver may attempt to recover the packet sent on each of Channels 1 and 4 based on all data symbol blocks received for that packet. The receiver may be able to recover the packet transmitted on, e.g., Channel 1 next, and would then estimate and cancel the interference due to this packet. In each cycle thereafter, the receiver may attempt to recover the packet sent on Channel 4 based on all data symbol blocks received for that packet. The receiver can thereafter simply cycle through the four parallel channels in a predetermined order, i.e., Channels 2, 3, 1, 4, then back to 2, and so on. This predetermined order is selected based on the order in which the packets are recovered for the four parallel channels. Whenever a data packet is recovered on the current parallel channel (the channel to attempt recovery first in the cycle), a new data packet is transmitted on that channel, and this packet is then recovered last.

[00106] The cycled SIC transmission scheme can provide good performance even with a crude rate selection. This is because IR transmission is effectively achieved for each data stream, as shown in FIGS. 9A and 9B. The cycled SIC transmission can provide good performance even if the channel conditions vary rapidly. Moreover, implementation of the cycled SIC transmission scheme is relatively simple since (1) the transmitter and receiver do not need to maintain state information for what is currently being transmitted and (2) the packet sizes do not need to be varied to fit within specific time windows, as is the case for the ordered SIC transmission scheme.

[00107] The ordered and cycled SIC transmission schemes are two exemplary schemes. Other transmission schemes may also be implemented for inter-dependent parallel channels. As an example, in a “hybrid” SIC transmission scheme, the receiver attempts to recover each of the data packets transmitted currently for the N_D data streams based on all data symbol blocks received for that packet (i.e., the receiver does not skip the decoding of any packet). Each data symbol block for each packet would have (1) the interference from recovered packets canceled and (2) interference from packets not yet recovered. The SINR for each data packet may thus vary across the entire packet, depending on the extent of the interference cancellation, if any, for the packet. The hybrid SIC transmission scheme may also be used in combination with the ordered and cycled SIC transmission schemes. For example, the receiver may attempt to recover the data packet on Channel 2 in each cycle after the first data packet on Channel 1 has been received and canceled (e.g., for each cycle after cycle N_{rec}^{1a} in FIGS. 6B and 6C).

3. Transmitter

[00108] FIG. 10 shows a block diagram of an embodiment of TX data processor 120 within transmitter 110. TX data processor 120 includes N_D TX channel data processors 1010a through 1010n for N_D data streams. Each TX channel data processor 1010 receives a respective data stream, processes each data packet in the data stream based on the rate selected for the stream, and provides a set of data symbol blocks for the packet. FIG. 11 illustrates the processing of one data packet by one data processor 1010.

[00109] Within each TX channel data processor 1010, a cyclic redundancy check (CRC) generator 1012 receives a data packet on the data stream being processed by data processor 1010, generates a CRC value for the data packet, and appends the CRC value to the end of the data packet to form a formatted packet. The CRC value is used by the receiver to check whether the packet is decoded correctly or in error. Other error detection codes may also be used instead of CRC. A forward error correction (FEC) encoder 1014 then encodes the formatted packet in accordance with a coding scheme or code rate indicated by the selected rate and provides a coded packet or “codeword”. The encoding increases the reliability of the packet transmission. FEC encoder 1014 may implement a block code, a convolutional code, a Turbo code, some other code, or a combination thereof. In FIG. 11, the coded packet includes a first portion with

systematic bits for the formatted packet, a second portion with parity bits from a first constituent encoder of a Turbo encoder, and a third portion with parity bits from a second constituent encoder of the Turbo encoder.

[00110] A partitioning unit 1016 receives and partitions the coded packet into N_B coded subpackets, where N_B may be dependent on the selected rate and indicated by a partitioning control from controller 180. The first coded subpacket typically contains all of the systematic bits and zero or more parity bits. This allows the receiver to recover the data packet with just the first coded subpacket under favorable channel conditions. The other $N_B - 1$ coded subpackets contain the remaining parity bits, with each subpacket typically containing parity bits taken across the entire data packet.

[00111] A channel interleaver 1020 includes N_B block interleavers 1022a through 1022nb that receive the N_B coded subpackets from partitioning unit 1016. Each block interleaver 1022 interleaves (i.e., reorders) the code bits for its subpacket in accordance with an interleaving scheme and provides an interleaved subpacket. The interleaving provides time, frequency, and/or spatial diversity for the code bits. A multiplexer 1024 couples to all N_B block interleavers 1022a through 1022nb and provides the N_B interleaved subpackets, one at a time and if directed by an IR transmission control from controller 180. Multiplexer 1024 provides the interleaved subpacket from block interleaver 1022a first, then the interleaved subpacket from block interleaver 1022b next, and so on, and the interleaved subpacket from block interleaver 1022nb last. Multiplexer 1024 provides the next interleaved subpacket if a NAK is received for the data packet. All N_B block interleavers 1022a through 1022nb can be purged whenever an ACK is received.

[00112] A symbol mapping unit 1026 receives the interleaved subpackets from channel interleaver 1020 and maps the interleaved data in each subpacket to modulation symbols. The symbol mapping is performed in accordance with a modulation scheme indicated by the selected rate. The symbol mapping may be achieved by (1) grouping sets of B bits to form B-bit binary values, where $B \geq 1$, and (2) mapping each B-bit binary value to a point in a signal constellation having 2^B points. This signal constellation corresponds to the selected modulation scheme, which may be BPSK, QPSK, 2^B -PSK, 2^B -QAM, and so on. As used herein, a “data symbol” is a modulation symbol for data, and a “pilot symbol” is a modulation symbol for pilot. Symbol

mapping unit 1026 provides a block of data symbols for each coded subpacket, as shown in FIG. 11.

[00113] For each data packet, TX channel data processor 1010 provides N_B data symbol blocks, which collectively include N_{SYM} data symbols and can be denoted as $\{s\} = [s_1 \ s_2 \ \dots \ s_{N_{SYM}}]$. Each data symbol s_i , where $i = 1 \dots N_{SYM}$, is obtained by mapping B code bits as follows: $s_i = \text{map}(\underline{b}_i)$ where $\underline{b}_i = [b_{i,1} \ b_{i,2} \ \dots \ b_{i,B}]$.

[00114] FIG. 12 shows a block diagram of an embodiment of TX spatial processor 130 and transmitter unit 132. TX spatial processor 130 receives and processes N_D data symbol streams from TX data processor 120 and provides N_T transmit symbol streams to transmitter unit 132. The processing by TX spatial processor 130 is dependent on the particular transmission scheme selected for use.

[00115] Within TX spatial processor 130, a matrix multiplication unit 1220 receives up to N_D data symbol blocks (represented by data vector \underline{s}) for each slot. Unit 1220 performs matrix multiplication of the data vector \underline{s} with (1) the unitary matrix \underline{V} for the second transmission scheme and (2) the transmit basis matrix \underline{M} for the third transmission scheme. Unit 1220 simply passes the data vector \underline{s} through for the other transmission schemes. A multiplexer/demultiplexer (MUX/DEMUX) 1222 receives the symbols from unit 1220 and provides these symbols to the proper transmit antennas and subbands (if OFDM is used). Multiplexer/demultiplexer 1222 also multiplexes in pilot symbols (e.g., in a time division multiplex (TDM) manner) and provides N_T transmit symbol sequences for the N_T transmit antennas in each slot. Each transmit symbol sequence is designated for transmission from one transmit antenna in one slot.

[00116] Transmitter unit 132 includes N_T OFDM modulators 1230a through 1230t and N_T TX RF units 1236a through 1236t for the N_T transmit antennas. For a single-carrier MIMO system, OFDM modulators 1230 are not needed, and TX spatial processor 130 provides the N_T transmit symbol sequences directly to TX RF units 1236a through 1236t. For a MIMO-OFDM system, TX spatial processor 130 provides the N_T transmit symbol sequences to OFDM modulators 1230a through 1230t. Each OFDM modulator 1230 includes an inverse fast Fourier transform (IFFT) unit 1232 and a cyclic prefix generator 1234. Each OFDM modulator 1230 receives a respective transmit symbol sequence from TX spatial processor 130 and groups each set of N_F transmit symbols and zero signal values for the N_F subbands. (Subbands not used for data

transmission are filled with zeros.) IFFT unit 1232 transforms each set of N_F transmit symbols and zeros to the time domain using an N_F -point inverse fast Fourier transform and provides a corresponding transformed symbol that contains N_F chips. Cyclic prefix generator 1234 repeats a portion of each transformed symbol to obtain a corresponding OFDM symbol that contains $N_F + N_{cp}$ chips. The repeated portion is referred to as a cyclic prefix, and N_{cp} is the number of chips being repeated. The cyclic prefix ensures that the OFDM symbol retains its orthogonal properties in the presence of multipath delay spread caused by frequency selective fading (i.e., a frequency response that is not flat). Cyclic prefix generator 1234 provides a sequence of OFDM symbols for the sequence of transmit symbols.

[00117] TX RF units 1236a through 1236t receive and condition N_T OFDM/transmit symbol sequences to generate N_T modulated signals, which are transmitted from N_T transmit antennas 1240a through 1240t, respectively.

4. Receiver

[00118] FIG. 13 shows a block diagram of a receiver 150a, which is one embodiment of receiver 150 in FIG. 1. At receiver 150a, N_R receive antennas 1310a through 1310r receive the N_T modulated signals transmitted by transmitter 110 and provide N_R received signals to N_R RX RF units 1312a through 1312r, respectively, within receiver unit 154. Each RX RF unit 1312 conditions and digitizes its received signal and provides a stream of symbols/chips. For a single-carrier MIMO system, OFDM demodulators 1314a through 1314r are not needed, and each RX RF unit 1312 provides a stream of symbols directly to a respective demultiplexer 1316. For a MIMO-OFDM system, each RX RF unit 1312 provides a stream of chips to a respective OFDM demodulator 1314. Each OFDM demodulator 1314 performs OFDM demodulation on its stream of chips by (1) removing the cyclic prefix in each received OFDM symbol to obtain a received transformed symbol and (2) transforming each received transformed symbol to the frequency domain with a fast Fourier transform (FFT) to obtain N_F received symbols for the N_F subbands. For both systems, demultiplexers 1316a through 1316r receive N_R symbol streams from RX RF units 1312 or OFDM demodulators 1314, provide N_R sequences of received symbols (for data) for each slot to RX spatial processor 160a, and provide received pilot symbols to channel estimator 172.

[00119] RX spatial processor 160a includes a detector 1320 and a multiplexer/demultiplexer 1322. Detector 1320 performs spatial or space-time processing (or “detection”) on the N_R received symbol sequences to obtain N_T detected symbol sequences for each slot. Each detected symbol is an estimate of a data symbol transmitted by the transmitter. Detector 1320 may implement an MRC detector shown in equation (2), an MMSE detector shown in equation (3), a linear zero-forcing detector shown in equation (4), an MMSE linear equalizer, a decision feedback equalizer, or some other detector/equalizer. The detection may be performed based on an estimate of the channel response matrix $\underline{\mathbf{H}}$ or the effective channel response matrix $\underline{\mathbf{H}}_{eff} = \underline{\mathbf{H}}\underline{\mathbf{M}}$, depending on whether or not the data symbols are pre-multiplied with the transmit basis matrix $\underline{\mathbf{M}}$ at the transmitter. For a MIMO-OFDM system, the receiver performs detection separately for each of the subbands used for data transmission.

[00120] For each slot, detector 1320 provides N_T detected symbol sequences that correspond to the N_T entries of $\hat{\underline{\mathbf{s}}}$. Multiplexer/demultiplexer 1322 receives the N_T detected symbol sequences and provides the detected symbols to N_D detected symbol blocks for the N_D data streams. Each detected symbol block is an estimate of a data symbol block transmitted by the transmitter.

[00121] Channel estimator 172 estimates the channel response matrix $\underline{\mathbf{H}}$ for the MIMO channel and the noise floor at the receiver (e.g., based on received pilot symbols) and provides channel estimates to controller 180. Within controller 180, a matrix computation unit 176 derives the detector response $\underline{\mathbf{W}}$ (which may be $\underline{\mathbf{W}}_{mrc}$, $\underline{\mathbf{W}}_{mmse}$, $\underline{\mathbf{W}}_{zf}$, or $\underline{\Sigma}^{-1}\underline{\mathbf{U}}^H$) based on the estimated channel response matrix, as described above, and provides the detector response to detector 1320. Detector 1320 pre-multiplies the vector $\underline{\mathbf{r}}$ of received symbols with the detector response $\underline{\mathbf{W}}$ to obtain the vector $\hat{\underline{\mathbf{s}}}$ of detected symbols. Rate selector 174 (which is implemented by controller 180 for the embodiment shown in FIG. 13) performs rate selection based on the channel estimates. A look-up table (LUT) 184 stores a set of rates supported by the MIMO system and a set of parameter values for each rate (e.g., the data rate, packet size, coding scheme or code rate, modulation scheme, and so on for each rate). Rate selector 174 accesses LUT 184 for information used for rate selection.

[00122] FIG. 14 shows a block diagram of an RX data processor 170a, which is one embodiment of RX data processor 170 in FIGS. 1 and 13. RX data processor 170a

includes N_D RX channel data processors 1410a through 1410n for N_D data streams. Each RX channel data processor 1410 receives and processes a respective detected symbol stream and provides a decoded data stream.

[00123] Within each RX channel data processor 1410, a symbol demapping unit 1430 receives detected symbol blocks from RX spatial processor 160a, one block at a time. For each detected symbol block, symbol demapping unit 1430 demodulates the detected symbols in accordance with the modulation scheme used for that block (as indicated by a demodulation control from controller 180) and provides a demodulated data block to a channel deinterleaver 1440. Channel deinterleaver 1440 includes a demultiplexer 1442 and N_B block deinterleavers 1444a through 1444nb. Prior to receiving a new data packet, block deinterleavers 1444a through 1444nb are initialized with erasures. An erasure is a value that substitutes for a missing code bit (i.e., one not yet received) and is given appropriate weight in the decoding process. Multiplexer 1442 receives demodulated data blocks from symbol demapping unit 1430 and provides each demodulated data block to the proper block deinterleaver 1444. Each block deinterleaver 1444 deinterleaves the demodulated data in its block in a manner complementary to the interleaving performed at the transmitter for that block.

[00124] For independent parallel channels, whenever a new data symbol block is received from the transmitter for a data packet on a parallel channel, the decoding can be performed anew on all blocks received for that packet. A re-assembly unit 1448 forms a packet of deinterleaved data for subsequent decoding. The deinterleaved data packet contains (1) deinterleaved data blocks for all data symbol blocks received for the current packet to be decoded and (2) erasures for data symbol blocks not received for the current packet. Re-assembly unit 1448 performs re-assembly in a complementary manner to the partitioning performed by the transmitter, as indicated by a re-assembly control from controller 180. An FEC decoder 1450 decodes the deinterleaved data packet in a manner complementary to the FEC encoding performed at the transmitter, as indicated by a decoding control from controller 180. For example, a Turbo decoder or a Viterbi decoder may be used for FEC decoder 1450 if Turbo or convolutional coding, respectively, is performed at the transmitter. FEC decoder 1450 provides a decoded packet for the current packet. A CRC checker 1452 checks the decoded packet to determine whether the packet is decoded correctly or in error and provides the status of the decoded packet.

[00125] FIG. 15 shows a block diagram of a receiver 150b, which implements the SIC technique and is another embodiment of receiver 150 in FIG. 1. Receiver 150b includes an RX spatial processor 160b and an RX data processor 170b that collectively implement N_D successive (i.e., cascaded) receiver processing stages. Each of stages 1 to $N_D - 1$ includes a detector 1510, an interference canceller 1520, an RX channel data processor 1530, and a TX channel data processor 1540. The last stage N_D includes only a detector 1510n and an RX channel data processor 1530n.

[00126] For stage 1, detector 1510a performs detection on the N_R received symbol sequences for each slot and provides a detected symbol block for a data packet (Packet x) in the data stream being recovered by stage 1. RX channel data processor 1530a demodulates, deinterleaves, and decodes all detected symbol blocks received for Packet x . If Packet x is decoded correctly, then TX channel data processor 1540a encodes, interleaves, and modulates Packet x to obtain a remodulated symbol sequence, which is an estimate of the data symbol sequence for Packet x . TX channel data processor 1540a performs the same processing as that performed by the transmitter for Packet x . Interference canceller 1520a receives and spatially processes the remodulated symbol sequence in the same manner performed by transmitter 110 for Packet x to obtain N_T transmit symbol sequences, which contain only the symbol components for Packet x . Interference canceller 1520a further processes the transmit symbol sequences with the channel response matrix to obtain interference components due to Packet x . The interference components are then subtracted from the N_R received symbol sequences to obtain N_R modified symbol sequences, which are provided to stage 2.

[00127] Each of stages 2 through $N_D - 1$ performs the same processing as stage 1, albeit on the N_R modified symbol sequences from the preceding stage instead of the N_R received symbol sequences. Stage N_D performs detection and decoding on the N_R modified symbol sequences from stage $N_D - 1$ and does not perform interference estimation and cancellation.

[00128] Detectors 1510a through 1510n may each implement an MRC detector, an MMSE detector, a linear zero-forcing detector, an MMSE linear equalizer, a decision feedback equalizer, or some other detector/equalizer. Each RX channel data processor 1530 may be implemented as shown in FIG. 14, and each TX channel data processor 1540 may be implemented as shown in FIG. 10. As described above, the receiver may attempt to recover the data packet for a later stage only after the data packets for earlier

stages have been recovered. Buffers (not shown in FIG. 15) would then store the symbols from each stage until they are ready for processing by later stages.

[00129] For both single-carrier MIMO and MIMO-OFDM systems, the receiver and/or transmitter can estimate the received SINRs or the post-processed SINRs (depending on whether or not SIC is used) for the N_D parallel channels and select a suitable rate for data transmission on each parallel channel. The rate selection may be performed in various manners. In one rate selection scheme, the rate for each parallel channel is selected based on the SINR needed by an equivalent system with an AWGN channel (i.e., with a flat frequency response) to support the average spectral efficiency computed for the parallel channel. This rate selection scheme is described in detail in commonly assigned U.S. Patent Application Serial No. 10/176,567, entitled "Rate Control for Multi-Channel Communication Systems," filed June 20, 2002. In another rate selection scheme, the rate for each parallel channel is selected based on an operating SINR computed for the parallel channel based on an average post-processed SINR for the parallel channel and an SINR offset. The highest rate with a required SINR (in an AWGN channel) that is less than or equal to the operating SINR is selected for the parallel channel. This rate selection scheme is described in detail in commonly assigned U.S. Patent Application Serial No. 10/394,529, entitled "Transmission Mode Selection for Data Transmission in a Multi-Channel Communication System," filed March 20, 2003.

[00130] The IR transmission techniques described herein may be implemented in a frequency division duplex (FDD) system and a time division duplex (TDD) system. For an FDD system, the forward MIMO channel and the feedback channel use different frequency bands and are likely to observe different channel conditions. In this case, the receiver can estimate the N_D parallel channels, select the rates for the parallel channels, and send back the selected rates, as shown in FIGS. 1 through 3. For a TDD system, the forward MIMO channel and the feedback channel share the same frequency band and are likely to observe similar channel conditions. In this case, the transmitter can estimate the N_D parallel channels based on a pilot sent by the receiver and selects the rates for the parallel channels. The channel estimation and rate selection may thus be performed by the receiver, the transmitter, or both.

[00131] The IR transmission techniques described herein may be implemented by various means. For example, these techniques may be implemented in hardware,

software, or a combination thereof. For a hardware implementation, the processing units used at the transmitter for IR transmission may be implemented within one or more application specific integrated circuits (ASICs), digital signal processors (DSPs), digital signal processing devices (DSPDs), programmable logic devices (PLDs), field programmable gate arrays (FPGAs), processors, controllers, micro-controllers, microprocessors, other electronic units designed to perform the functions described herein, or a combination thereof. The processing units used at the receiver for receiving an IR transmission may also be implemented within one or more ASICs, DSPs, DSPDs, PLDs, FPGAs, processors, controllers, and so on.

[00132] For a software implementation, the IR transmission techniques may be implemented with modules (e.g., procedures, functions, and so on) that perform the functions described herein. The software codes may be stored in a memory unit (e.g., memory units 142 and 182 in FIG. 1) and executed by a processor (e.g., controllers 140 and 180). The memory unit may be implemented within the processor or external to the processor, in which case it can be communicatively coupled to the processor via various means as is known in the art.

[00133] Headings are included herein for reference and to aid in locating certain sections. These headings are not intended to limit the scope of the concepts described therein under, and these concepts may have applicability in other sections throughout the entire specification.

[00134] The previous description of the disclosed embodiments is provided to enable any person skilled in the art to make or use the present invention. Various modifications to these embodiments will be readily apparent to those skilled in the art, and the generic principles defined herein may be applied to other embodiments without departing from the spirit or scope of the invention. Thus, the present invention is not intended to be limited to the embodiments shown herein but is to be accorded the widest scope consistent with the principles and novel features disclosed herein.

[00135] WHAT IS CLAIMED IS: